

Wideband Printed Monopole Antenna for Application in Wireless Communication Systems

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Abstract –Empirical results of an electrically small printed monopole antenna is described with fractional bandwidth of 185% (115 MHz–2.90 GHz) for return-loss better than 10 dB, peak gain and radiation efficiency at 1.45 GHz of 2.35 dBi and 78.8%, respectively. The antenna geometry can be approximated to a back-to-back triangular shaped patch structure that is excited through a common feed-line with a meander-line T-shape divider. The truncated ground-plane includes a central stub located underneath the feed-line. The impedance bandwidth of the antenna is enhanced with the inclusion of meander-line slots in the patch and four double split-ring resonators on the underside of the radiating patches. The antenna radiates approximately omnidirectionally to provide coverage over a large part of VHF, whole of UHF, entire of L-band and some parts of S-band. The antenna has dimensions of $48.32 \times 43.72 \times 0.8$ mm³, which is corresponding with the electrical size of $0.235\lambda_0 \times 0.211\lambda_0 \times 0.003\lambda_0$, where λ_0 is free-space wavelength at 1.45 GHz. The proposed low-profile low-cost antenna is suitable for application in wideband wireless communications systems.

Keywords – Printed monopole antenna, wideband antenna, truncated ground plane, back-to-back triangular shaped radiation patch, split ring resonators (SRR).

1. INTRODUCTION

Advanced modern wireless systems incorporate various radio frequency technologies such as WiFi, WiMAX, Zigbee, 3G and LTE. The antennas for these systems therefore need to satisfy stringent requirements including wide impedance bandwidth, omnidirectional radiation, stable gain and radiation pattern, and low profile design [1]-[6]. In the past decades, tremendous research has been carried out to achieve various design objectives. Several wideband low profile antennas have been designed by employing slot antenna [7]-[10], loop antenna [11], [12] and spiral antenna [13]-[15]. Electromagnetic band-gap (EBG) structure, which is an artificial electromagnetic material, has been used to

reduce the antenna dimensions to less than $0.1\lambda_0$. This has been demonstrated by locating a dipole antenna [16] or a folded dipole antenna [17] or a spiral antenna [18] on a carefully designed EBG structure. Essentially, the operating bandwidth of the antenna is limited by the bandwidth of the reflection phase of the EBG surface; hence wideband antennas cannot be excited on the EBG surface.

Microstrip patch antenna is an alternative solution to achieve a low-profile design, which has many advantages, such as planar structure, low cost, and ease of manufacture. However, conventional patch antennas [19] suffer from very narrow impedance bandwidth (less than 5%), which therefore cannot fulfill the bandwidth requirement of the modern wireless system. Numerous

bandwidth enhancement techniques have been reported to date, such as the L-probe feed [20], [21], coplanar coupled feed [22], aperture coupled feed [23], stacked patches [24], U-slot patch [25], E-shaped patch [26] and chorded crescent shaped patch [27]. With these techniques the impedance bandwidth has been greatly enhanced by up to 50% for $VSWR \leq 2$. However, the radiation patterns of these patch antennas vary with frequency, and they can suffer from high cross-polarization and strong back radiation across their operating frequency range.

In this paper, a novel wideband printed monopole antenna structure is reported. The antenna is composed of back-to-back triangular shaped radiating patches that are excited through a common feed-line. The ground-plane of the antenna is a truncated T-shaped structure that is located under the feed-line. Etched in the patches is a meandered slot line, and embedded under the two patches are four double split-ring resonators. These elements stretch regions of well-matched impedance and therefore enhance the antenna's impedance bandwidth. The proposed antenna radiates approximately omnidirectionally over 115 MHz - 2.90 GHz. The antenna is compact with dimensions of $0.235\lambda_0 \times 0.211\lambda_0 \times 0.003\lambda_0$ at 1.45 GHz that enables easy integrated with RF front-end circuitry.

2. ANTENNA DESIGN

This section is devoted to describe the antenna design concept. The initial antenna design starts from Antenna#1. Then, by inserting meandered line slot into the tree-shaped patches, Antenna#2 is formed to improve the radiation characteristics of Antenna#1. To further improve the impedance bandwidth of the Antenna#2, then three split-ring resonators (SRR) are loaded on the bottom side of the antenna substrate to form antenna#3 and then four SSRs are added to form the final model of antenna#4. These antennas were constructed on Rogers/RT Duroid 5880 substrate with dielectric constant of 2.2, thickness of 0.8 mm, and loss-tangent of 0.0009. The detailed discussion of these antennas will be given the following sub-sections.

2.1 Antenna#1

Geometry of the first version of this proposed antenna shown in Fig. 1(a), is constituted from two identical back-to-back printed patches that be approximated to a

triangular shape or can be considered to resemble a tree like structure. The tree-shaped patches are placed in close proximity to each other and fed through a common feed-line through a T-shape divider. On the bottom side of the antenna substrate is a truncated ground-plane with a stub, as shown in Fig.1(b). All the dimension of the antenna was given in Table 1. Dimensions of the two-identical back-to-back printed patches are based on an approximation for a triangular microstrip antenna whose resonant frequencies were obtained from cavity model with perfect magnetic walls given by [28]:

$$f_{mn} = \frac{2c}{3a\sqrt{\epsilon_r}} [m^2 + mn + n^2]^{1/2} \quad (1)$$

where c is the velocity of electromagnetic waves in free space, ϵ_r is the relative dielectric constant of the substrate, m and n are the integers which refer to TM modes, and a is the length of a side of the triangle.

The antenna structure was simulated using High Frequency Structure Simulator (HFSS), which is a full wave electromagnetic simulator. From the simulation response of Antenna#1, shown in Fig. 2, it is discernible that the antenna exhibits two visible notched-bands. The bandwidth and gain of Antenna#1 are given in Table 2. To eliminate these notched bands, the T-junction of the feed-line connecting the tree-shaped patches is meandered and a ground-plane stub is added on the bottom side of the substrate. The ground-plane, shown in Fig. 1(b), now resembles a T-shape structure where the ground stub is located underneath the feed-line. Careful design of the meandered line (ML) T-shaped junction and ground-plane stub eliminate the notched bands, which is evident in Fig. 2.

The ML and ground stub also improve the impedance matching from $S_{11} \leq -18\text{dB}$ to -20dB , however the resonance frequency is shifted from 1.47 GHz to 1.40 GHz with 28% reduction in the impedance bandwidth. Fig. 3 shows the measured gain and efficiency performance of Antenna#1, and the salient results are given in Table 3. Maximum gain and efficiency at the resonance frequency of $f_r = 1.55$ GHz are 0.35 dBi and 22.8%, respectively. Table 4 compares simulated and measured impedance bandwidth, resonant frequency and return-loss. The discrepancies in the result are attributed to manufacturing tolerance and imperfect soldering of the SMA connector to the antenna feed-line.

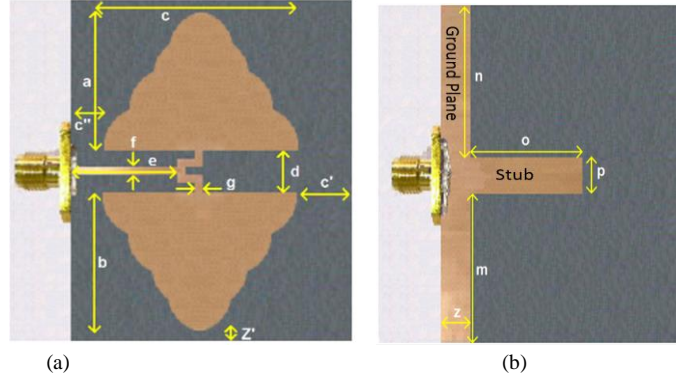


Fig. 1. Photograph of the proposed Antenna#1, (a) top side and (b) bottom side.

Table 1. Antenna parameter values in millimeters. Antenna size is: $48.32 \times 43.72 \times 0.8$ mm³ on Rogers/RT Duroid 5880.

a	b	c	d	e	f	g	h	i	j
19.48	19.48	31	6.36	16	1.4	1.5	2	2	2
k	l	m	n	o	p	z	z'	c'	c''
2.4	1.6	24	24	20	6	5.2	1.5	7.86	4.86

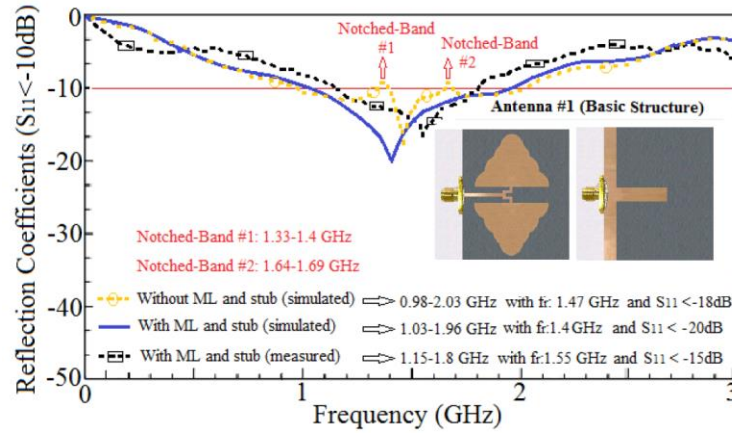


Fig. 2. Reflection coefficient response of Antenna#1.

Table 2. Bandwidth and gain of the band notches in Antenna#1

Band notch #1	$1.33 - 1.4 \text{ GHz} \rightarrow -0.14 \leq \text{Gain} \leq -0.05$
Band notch #2	$1.64 - 1.69 \text{ GHz} \rightarrow -0.82 \leq \text{Gain} \leq -0.03$

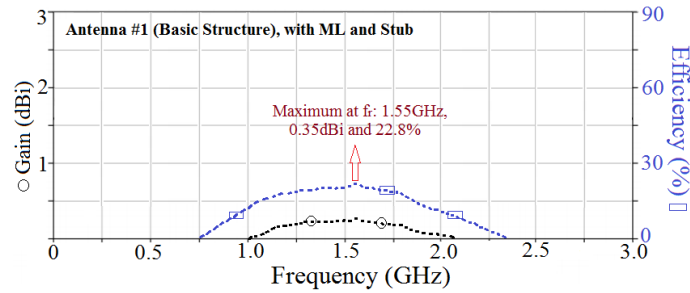


Fig. 3. Measured gain and efficiency response as a function of frequency of Antenna#1 (basic structure) with meandered line T-junction feed and ground-plane stub.

Table 3. Measured gain and efficiency performance of Antenna#1 with ML and ground stub

Frequency (GHz)	1.15	$f_r = 1.55$	1.8
Gain (dBi)	0.2	0.35	0.27
Efficiency (%)	17.35	22.8	19.58

Table 4. Simulated and measured impedance bandwidth, resonant frequency and return-loss of Antenna#1

Simulated freq. range (Fractional BW): 1.03 – 1.96 GHz (62.20%), $f_{r_{sim.}} = 1.4$ GHz and $S_{11_{sim.}}$ better than 20 dB
Measured freq. range (Fractional BW): 1.15 – 1.8 GHz (44.06%), $f_{r_{meas.}} = 1.55$ GHz and $S_{11_{meas.}}$ better than 15 dB

2.2 Antenna #2

To improve the radiation characteristics of Antenna#1 a meandered line slot was etched on both the tree-shaped patches, as shown in Fig. 4. The dimensions of the antenna parameters are given in Table 1. The reflection coefficient response of Antenna#2 in Fig. 5 shows improvement in the impedance bandwidth. Two new regions of well-matched impedance are produced by the additional slots at $f_{r1} = 1.33$ GHz and $f_{r3} = 1.75$ GHz.

The radiation pattern of the antenna was measured in a compact range anechoic chamber with a horn antenna transmitting spherical waves towards a reflector

that converted the incident waves to plane waves which were directed towards the proposed antenna under test. Fig. 6 show that Antenna#2 has a maximum gain and radiation efficiency of 2 dBi and 70%, respectively, at $f_{r3} = 1.75$ GHz. Other details are given in Table 5. This improvement is approximately four-fold that of Antenna#1. Table 6 compares simulated and measured impedance bandwidth, resonant frequency and return-loss. The discrepancies in the result are attributed to manufacturing tolerance and imperfect soldering of the SMA connector to the antenna feed-line.

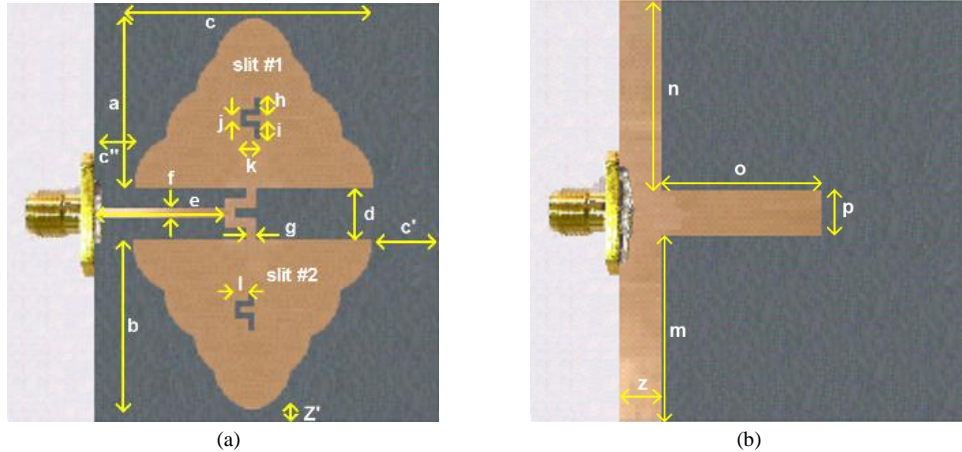


Fig. 4. Antenna#2 is essentially Antenna#1 with a meandered line etched on both patches, a) front view, b) back view.

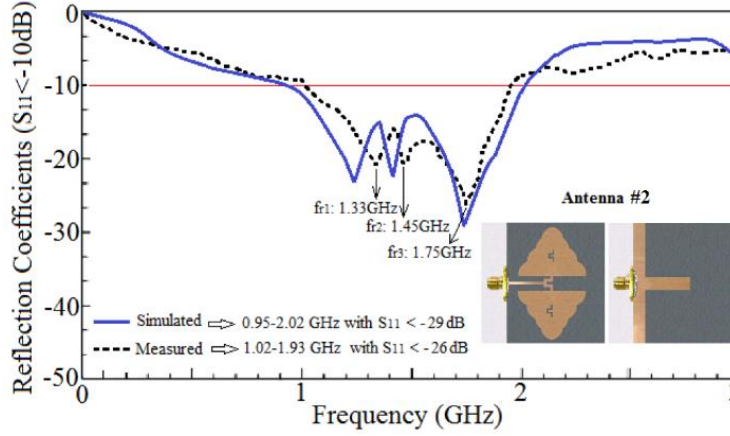


Fig. 5. Reflection coefficient response for Antenna#2.

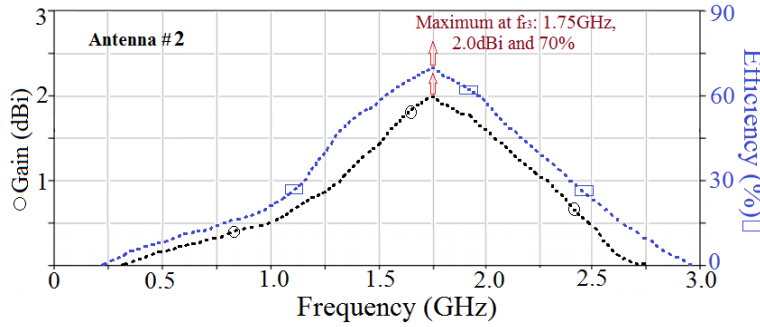


Fig. 6. Measured gain and efficiency response as a function of frequency for Antenna#2.

Table 5. Measured gain and efficiency performance of Antenna#2

Frequency (GHz)	1.02	$f_{r1} = 1.33$ (slot #2)	$f_{r2} = 1.45$ (ML and ground stub)	$f_{r3} = 1.75$ (slot #1)	1.93
Gain (dBi)	0.55	1.05	1.37	2.00	1.75
Efficiency (%)	22.82	47.11	56.26	70.00	62.48

Table 6. Simulated and measured impedance bandwidth, resonant frequency and return-loss of Antenna#2

Bandwidth and Fractional BW%	Simulated: 1.07 GHz from 0.95 – 2.02 GHz, 72.05%
	Measured: 0.91 GHz from 1.02 – 1.93 GHz, 61.69%
First resonance frequency	Simulated: 1.24 GHz for $ S_{11} \leq 23$ dB
	Measured: 1.33 GHz for $ S_{11} \leq 20$ dB
Second resonance frequency	Simulated: 1.42 GHz for $ S_{11} \leq 23$ dB
	Measured: 1.45 GHz for $ S_{11} \leq 20$ dB
Third resonance frequency	Simulated: 1.74 GHz for $ S_{11} \leq 29$ dB
	Measured: 1.75 GHz for $ S_{11} \leq 26$ dB

2.3 Antenna #3

Besides having a good radiation characteristic, it is important the antenna has a wide impedance bandwidth and good matching performance to provide suitable coverage over several communications standards. This was achieved by loading the bottom side of the antenna substrate with split-ring resonators (SRR), as shown in Fig. 7. At the operating frequency the magnetic-flux penetrating the SSR induces rotating currents in the

rings, which produce their own flux to enhance or oppose the incident field. Due to splits in the rings the structure can support resonant wavelengths much larger than the diameter of the rings. The small gaps between the rings creates a large capacitance that lowers the resonating frequency of the SRR. The dimensions of SRR are small compared to the resonant wavelength. The dimensions of the SRR are given in Table 7.

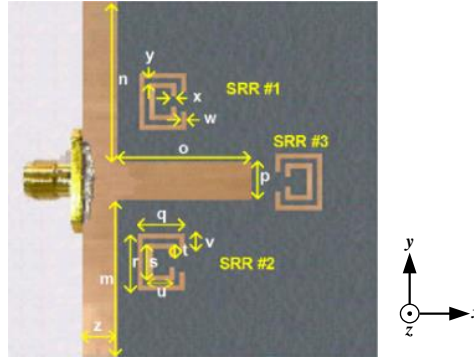


Fig. 7. Antenna#3, which is based on Antenna#1 includes three SRRs on the ground-plane; (Dimensions are given in Table 7).

Table 7. Split-ring resonator (SRR) parameter values in millimeters.

q	r	s	t	u	v	w	x	y
7.2	8.7	5.7	1.98	4	2.8	0.8	0.8	0.8

Reflection coefficient, gain and efficiency responses of Antenna#3 are shown in Figs. 8 and 9, and salient characteristics given in Table 8. By loading three SRRs resulted in three new regions of well-matched impedance centered at $f_{r4} = 1.85$ GHz, $f_{r5} = 2.15$ GHz, and $f_{r6} = 2.5$ GHz. SRRs extend the impedance bandwidth and improve the matching performance, however increase the radiation characteristics only moderately.

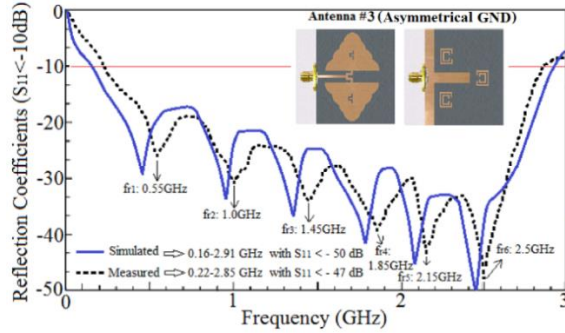


Fig. 8. Reflection coefficient response for Antenna#3.

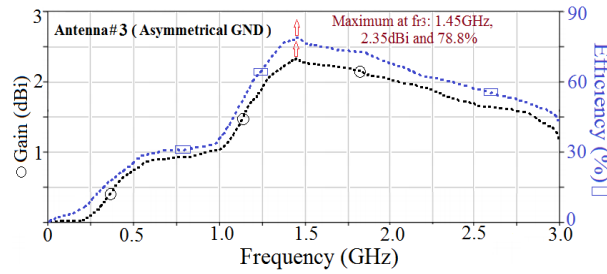
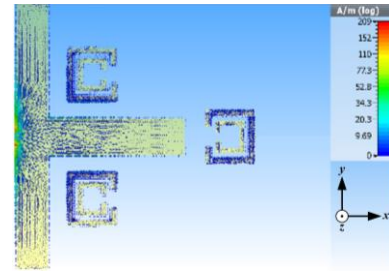
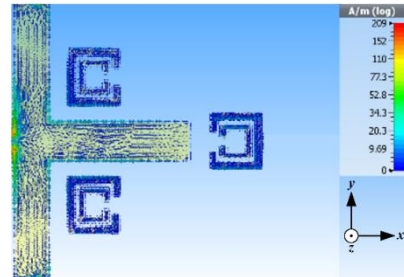


Fig. 9. Measured gain and efficiency as a function of frequency for Antenna#3.



@ $f_{r1} = 0.55$ GHz



@ $f_{r3} = 1.45$ GHz

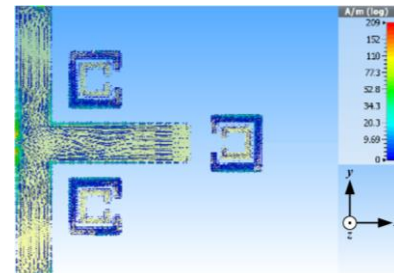


Table 8. Measured gain and efficiency performance of Antenna#3

Freq.(GHz)	0.22	$f_{r1} = 0.55$ (slot#2)	$f_{r2} = 1$ (ML & stub)	$f_{r3} = 1.45$ (slot#1)	$f_{r4} = 1.85$ (SRR#1)	$f_{r5} = 2.15$ (SRR#2)	$f_{r6} = 2.5$ (SRR#3)	2.85
Gain (dBi)	0.05	0.85	1.04	2.35	2.18	1.95	1.72	1.52
Eff. (%)	7.44	28.57	36.1	78.85	72.53	64.39	57.65	50.3

Table 9. Simulated and measured impedance bandwidth, resonant frequency and return-loss of Antenna#3

Bandwidth, Freq. range & Fractional BW%	Simulated: 2.75 GHz, 0.16 – 2.91 GHz, 179.15%
	Measured: 2.63 GHz, 0.22 – 2.85 GHz, 171.33%
1 st resonance frequency	Simulated: 0.46 GHz for $ S_{11} \leq 28$ dB
	Measured: 0.55 GHz for $ S_{11} \leq 25$ dB
2 nd resonance frequency	Simulated: 0.96 GHz for $ S_{11} \leq 33$ dB
	Measured: 1.0 GHz for $ S_{11} \leq 30$ dB
3 rd resonance frequency	Simulated: 1.35 GHz for $ S_{11} \leq 35$ dB
	Measured: 1.45 GHz for $ S_{11} \leq 32$ dB
4 th resonance frequency	Simulated: 1.79 GHz for $ S_{11} \leq 42$ dB
	Measured: 1.85 GHz for $ S_{11} \leq 38$ dB
5 th resonance frequency	Simulated: 2.08 GHz for $ S_{11} \leq 45$ dB
	Measured: 2.15 GHz for $ S_{11} \leq 44$ dB
6 th resonance frequency	Simulated: 2.45 GHz for $ S_{11} \leq 50$ dB
	Measured: 2.5 GHz for $ S_{11} \leq 47$ dB

Table 10. Wireless communication system frequencies covered by the proposed antenna.

System	Operating Frequency
Advanced Mobile Phone Service (AMPS)	824–894 MHz
Lower Band of Global System for Mobile Communications (GSM)	880–960 MHz
Personal Communication Service (PCS)	1.71–1.88 GHz
Upper Band of Global System for Mobile Communications (GSM)	1.85–1.99 GHz
Wideband Code Division Multiple Access (WCDMA)	1.92–2.17 GHz
Universal Mobile Telecommunication Systems (UMTS)	1.92–2.17 GHz
Personal Communication System (PCS)	1.85–1.99 GHz
Cellular	824–894 MHz
Digital Cellular System (DCS)	1.71–1.88 GHz
GSM900	890–960 MHz
International Mobile Telecommunication-2000 (IMT-2000)	1.92–2.17 GHz
CDMA450	411–493 MHz
JCDMA	832–925 MHz
KPCS	1.75–1.87 GHz
Global Position System (GPS)	1574.4–1576.4 MHz
Lower and upper bands of WiMAX	2.3–2.4 GHz and 2.496–2.690 GHz
Lower band of WiFi	2.412–2.4835 GHz
Bluetooth	2.402–2.480 GHz

@ $f_{r6} = 2.5$ GHz

Fig. 10. Surface current density distribution at spot frequencies.

Current density distribution over the ground-plane stub and split-ring resonators at various resonance frequencies, in Fig. 10, shows the current density is more pronounced at the mid-band frequency of 1.45 GHz. At this frequency (f_{r3}) the measured gain and efficiency of

Antenna#3 have an optimum value of 2.35 dBi and 78.8%, respectively.

Measured co- and cross-radiation patterns in E- and H-planes at its operating frequencies are given in Figs. 11 and 12. At $f_{r1} = 0.55$ GHz, $f_{r2} = 1.0$ GHz, $f_{r3} = 1.45$ GHz, and $f_{r6} = 2.5$ GHz, the cross-polarization radiation in E-plane is very low. Table 9 compares

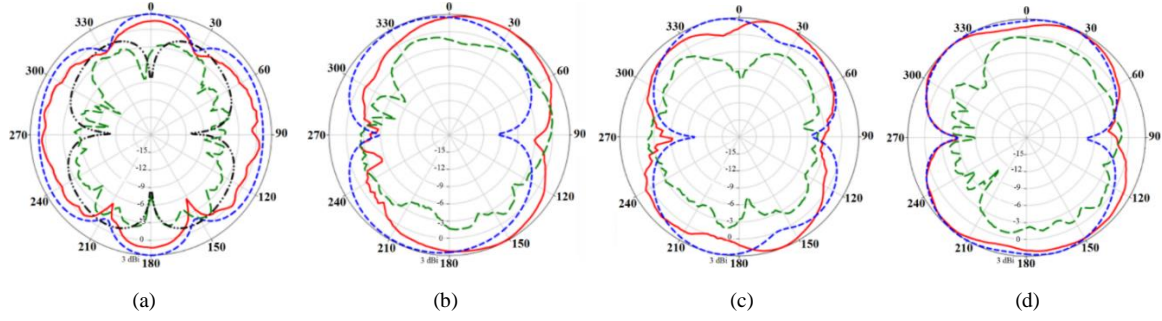


Fig. 11. Measured radiation patterns of the Antenna#3, a) at f : 220 MHz, b) at $fr1$: 550 MHz (ML-slit#2), c) at $fr2$: 1.0 GHz (ML and stub), d) at $fr3$: 1.45 GHz (ML-slit#1). Blue, red, black, and green lines represent co-pol at E-plane (z - x), co-pol at H-plane (z - y), cross-pol at E-plane, and cross-pol at H-planes, respectively.

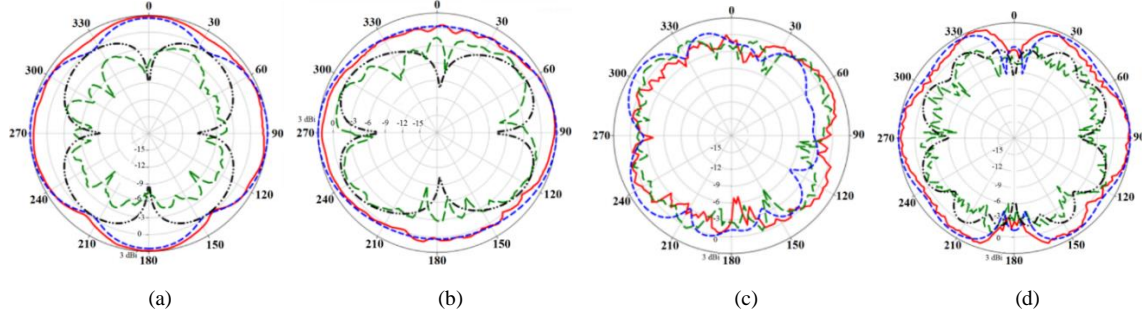


Fig. 12. Measured radiation patterns of the Antenna#3, a) at $fr4$: 1.85 GHz (SRR#1), b) at $fr5$: 2.15 GHz (SRR#2), c) at $fr6$: 2.5 GHz (SRR#3), d) at f : 2.85 GHz. Blue, red, black, and green lines represent co-pol at E-plane (z - x), co-pol at H-plane (z - y), cross-pol at E-plane, and cross-pol at H-planes, respectively.

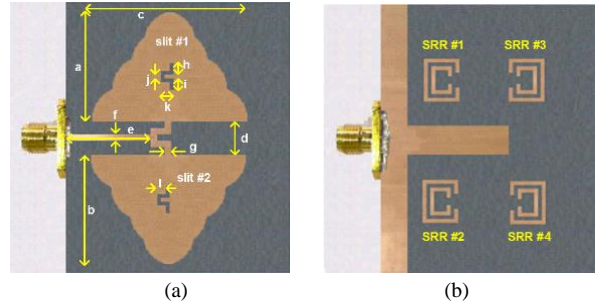


Fig. 13 Finalized antenna with symmetrically loaded ground-plane SRRs, a) front view, b) back view.

simulated and measured impedance bandwidth, resonant frequency and return-loss. Discrepancies in the result are attributed to manufacturing tolerance and imperfect soldering of the SMA connector to the antenna feed-line. The proposed antenna covers parts of VHF, whole of UHF, entire L-band and some parts of the S-band, as indicated in Table 10.

2.4 Antenna #4

To further enhance the impedance bandwidth of Antenna#3, the antenna was analyzed with four symmetrically located ground-plane split-ring resonators (SRR) shown in Fig. 13. Reflection coefficient response of this antenna, in Fig. 14, shows the creation of an

additional region of well matched impedance. As a result, there is improvement in the impedance bandwidth and matching. Simulated and measured fractional bandwidths are 188% and 180.32%, respectively.

3. PARAMETERIC STUDY

A parameter study was conducted to determine how the key parameters, i.e. ground stub, patch slit, and SRR, affected the performance of the antenna. Fig. 15(a) shows the effect of the ground stub length (o) and width (p) on the gain and radiation efficiency of the proposed antenna. It is clear from this graph that by increasing the length and width of the ground stub the antenna's effective aperture is increased, and the consequence of

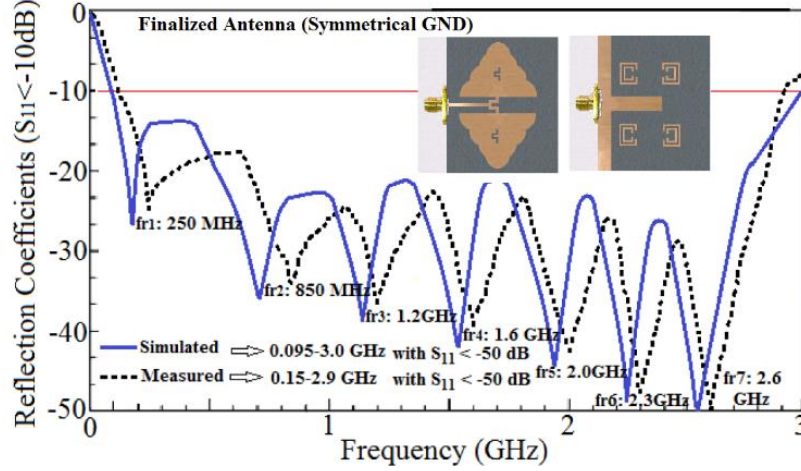


Fig. 14. Reflection coefficient response of the final antenna with four symmetrically located ground plane SRR.

this is enhanced antenna gain and efficiency performance. When ground stub length and width are increased from $o = 10$ mm and $p = 2$ mm to $o = 20$ mm and $p = 6$ mm, the gain and efficiency are increased by 1.1 dBi and 32.9% at 1.45 GHz, respectively.

The effect of number of the SRRs on the radiation characteristics are shown in Figs. 15(b) & (c). It is evident that by increasing the SRRs from one to three, the gain and efficiency correspondingly increase too. In fact, at 1.45 GHz the gain and efficiency increase by 0.36 dBi and 8.67%, respectively.

Fig. 15(d) show the effect of the patch slot on the gain and efficiency of the antenna. When the length and width of the slot are increased from 2 mm & 1 mm (initial case), respectively, to 6 mm & 2 mm (optimized case), the antenna's gain and efficiency improve by 0.23 dBi and 18.2%, respectively. The bandwidth is also enhanced by 17.3%. These results reveal the electromagnetic interaction between the patch and slot contribute in enhancing the antenna's performance. This is because a longer slot length effectively improves the impedance matching of the antenna. With this technique a smaller aperture is achieved with no compromise in the antenna's characteristics.

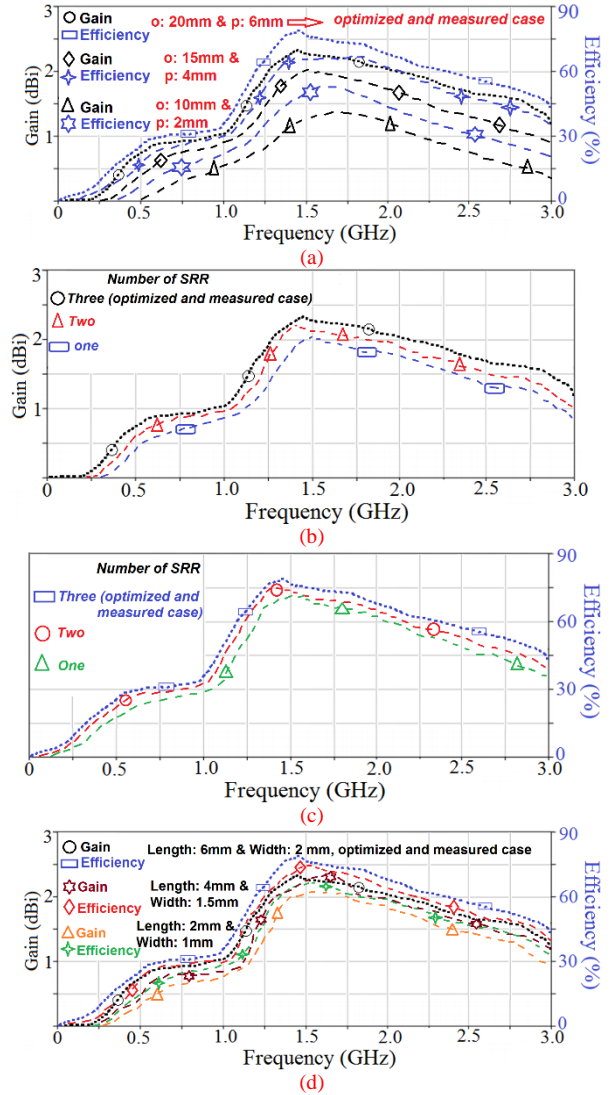


Fig. 15. Parametric study on the antenna's key parameters: a) length and width of the ground stub, b) number of SRRs on antenna gain, c) number of SRRs on antenna efficiency, and d) length and width of the patch slot.

4. COMPARISON OF THE PROPOSED ANTENNA

Comparison of the salient characteristics (i.e. freq. range, bandwidth, gain, radiation efficiency, and size) of the proposed antenna structure with other recently reported microstrip planar antennas is given in Table 11. The

proposed antenna exhibits a wide frequency range extending from 115 MHz to 2.90 GHz and therefore a large bandwidth performance with a relatively small foot print. Although its radiation efficiency is comparable with other antennas however its gain is relatively low.

Table 11. Comparison of the proposed antenna with the previous designs in the cited references for the freq. range, bandwidth, gain, radiation efficiency, and size.

References	Size (mm ³)	Freq. Range / [BW] (GHz)	Max. Gain (dBi)	Max. Efficiency (%)
[3]	100×50×9	Lower band: 0.88–0.91 [0.03] Upper band: 2.90–5.35 [2.45]	Lower band: 1.8 Upper band: 7	Lower band: - Upper band: -
[4]	13×24×1.6	3.10 – 4.50 [1.40]	6.0	50
[5]	60×80×0.8	0.60 – 3.00 (<i>several narrow bands</i>)	4.0	95
[6]	35×26×1.6	0.88–5.90 (<i>several narrow bands</i>)	5.27	81.3
[7]	80×101×1.5	2.24 – 2.66 [0.42]	5.2	95
[10]	56×50×1	2.36 – 2.49 [0.13]	-	80.8
[14]	51×28×1.524	Low band: 0.432 – 0.434 [0.002] High band: 2.38 – 2.50 [0.12]	Low band: 11.5 High band: 0.5	Low band: 7 High band: 72
[21]	50×50×3.81	2.72 - 3.17 [0.45]	7.0	-
[23]	100×100×9.6	1.50 – 2.60 [1.10]	6.4	-
[24]	47.59×31.86×8.27	1.00 – 1.30 [0.30]	6.0	-
[25]	70×42×28	0.75 – 1.00 [0.25]	8.0	-
[25]	45×70×10	2.10 – 3.00 [0.90]	9.5	-
[26]	145×127×1.59	0.78 – 0.94 [0.16]	12.5	-
This paper	48.32×43.72×0.8	0.115 – 2.90 [2.785]	2.35	78.85

5. CONCLUSION

Feasibility of a novel printed monopole antenna is demonstrated for wideband applications. The antenna is composed of back-to-back tree-shaped radiating patches on which is etched a meandered line slot and the ground-plane is loaded with four double split-ring resonators. The grounded-plane is a truncated T-shaped structure. These modifications to the antenna introduce additional regions of well matched impedance that enhance the antennas impedance bandwidth. The antenna exhibits a fractional bandwidth of 185% from 115 MHz–2.90 GHz for $|S_{11}| \leq -10$ dB with a peak gain of 2.35 dBi and radiation efficiency of 78.8% at 1.45 GHz. The antenna has dimensions of 48.32×43.72×0.8 mm³ that is equivalent to $0.235\lambda_0 \times 0.211\lambda_0 \times 0.003\lambda_0$, where λ_0 is free-space wavelength at the resonance frequency of 1.45 GHz. The antenna radiates approximately omnidirectionally. The measured and simulated results are in good agreement. Owing to the compact size, simple design and easy integration with RF front-end circuitry, the proposed antenna is attractive for use in wireless communication systems.

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